

# RECEIVING SYSTEMS FOR LOW LOSS BANDPASS FILTERS

ANAND K. S.

Low loss bandpass filters are being used extensively in receiving systems to compensate with deep space probes and to perform radio science experiments. They incorporate sensitive high-electron mobility transistors (HEMTs) or mesases with very low noise temperatures as their front-end amplifiers. Radio frequency interference (RFI) can significantly degrade the performance of these sensitive systems. Out-of-band RFI can result in gain compression, noise temperature increases, and in the case of mesases, spurious output signals.

Low loss bandpass filters fabricated from high temperature superconducting (HTS) materials can provide RFI protection for these amplifiers. The low loss that these filters exhibit allow them to provide protection without significantly degrading the noise temperature or insertion performance (return loss, group delay variation, etc.) of the receive system.

Superconducting technologies incorporated in Santa Barbara, Cal. formula, designed and fabricated a 2.3 GHz (W-band) and a 8.45 GHz (X-band) bandpass filters for HTS. Both prototype filters incorporate a five-resonator, all-phiine structure with  $\pi$ -Coupled  $\text{Cu-O}$  thin film resonator. They were designed to have a bandwidth of 60 MHz and 150 MHz, respectively, with a desired insertion loss of less than 0.5 dB.

The losses are minimized by CR at 12.16V/100V, i.e. at the end of cycle cell open. The lowest insertion loss is  $0.11$  dB for  $0.21$  dB/inch  $^{1/2}$  in  $^{1/2}$  (factor 10 spec) with a return loss of about 15 dB. The insertion loss appears to be  $0.11$  dB only if infinite factors of 10 return losses and impedances are used, it is not by the copper matching network losses.

## Introduction

The Jet Propulsion Laboratory (JPL) uses extremely sensitive receive systems to communicate with deep space probes and to perform radio science experiments. Radio frequency interference (RFI) can significantly degrade the receive system performance. Low loss bandpass filters fabricated from High Temperature Superconducting (HTS) materials will provide out of band RFI protection for HEMT low noise receivers without degrading their noise and microwave performance. The objective of this work is to demonstrate HTS RFI filters for cryogenic HEMT LNAs at 2.3 and 8.45 GHz.

### Insertion Loss Measurements

An automatic microwave network analyzer test set was used to measure the insertion and return loss of the filters (see figure 1). To measure the losses at 12 K the filters and the necessary microwave circuits were cooled in a two stage closed cycle refrigerator (CCR).

Two **low loss** 40 mm coaxial transmission lines with APC7

with end on signal. Let  $P_{in}$  be the input power to the system,  $P_{out}$  the output power, and  $P_{loss}$  the power lost to the environment. The input power is  $P_{in} = V_{in} I_{in}$ , the output power is  $P_{out} = V_{out} I_{out}$ , and the power lost to the environment is  $P_{loss} = V_{loss} I_{loss}$ .

$$P_{in} = P_{out} + P_{loss} \quad (1)$$

$$V_{in} I_{in} = V_{out} I_{out} + V_{loss} I_{loss} \quad (2)$$

The noise sources are amplified by a factor  $G$ , which is the gain of the system. The noise power is converted and detected by a power meter (see figure 2). The ratio of measured noise power to the input power into the following expression to obtain the receiver noise temperature  $T_n$ :

$$P_n = k_B T_n B \quad (3)$$

where  $k_B$  is Boltzmann's constant,  $T_n$  is the noise temperature of the device,  $B$  is the bandwidth of the system, and  $P_n$  is the noise power with load to the noise power with cold load.

The insertion loss of the filter is 0.17 dB at 2.3 GHz and 0.24 dB at 8.45 GHz. However, the measured insertion loss is expected to be higher because the filter uses inverted metal SMT connectors which can contribute up to 0.2 dB of loss at 2.3 GHz.

The filters were designed to have a bandwidth of 60 MHz at S-band and 150 MHz at X-band with an in-band ripple of less than 0.05 dB for both. Using an optimistic estimate of the unloaded Q (-10,000) the midband insertion loss at 2.3 GHz is expected to be 0.17 dB, and 0.24 dB at 8.45 GHz. However, the measured insertion loss is expected to be higher because the filter uses inverted metal SMT connectors which can contribute up to 0.2 dB of loss at 2.3 GHz.

At 12 K the S-band filter exhibited a bandwidth of 75 with a passband peak-to-peak ripple of 0.874 dB. The maximum insertion loss of 1.07 dB corresponded exactly with the percent return loss, the 1.07 dB seen at 2.3 GHz. The filter has a 1.07 dB loss at 2.3 GHz.

and return loss results. However, at frequencies where the filter was well matched, the insertion loss was approximately 0.33 dB.

This being a prototype filter there were problems that occurred that caused the poor match near the center frequency. They arose because of stresses that damaged the substrate during its manufacturing. Those problems were solved for the X-band amplifier which is reasonably matched across the band.

The X-band filter exhibited a passband peak to peak ripple of 0.31 dB with a maximum insertion loss of -0.656 dB and a band width of 160 MHz. Figure 5 shows a plot of the insertion and return loss results for this filter.

Taking into account the losses contributed by the connectors the filter losses agree reasonably well with the measured results.

The filters' insertion loss as a function of temperature responses exhibited very similar responses. There was very little change in the insertion loss below 50 K while very dramatic changes were observed from 100-115 K to 50 K.

#### Noise Temperature Contribution

For an extremely low loss and reasonably matched filter the

The input is  $\mathbf{x} = [x_1, x_2, \dots, x_N]^T$  and the output is  $\mathbf{y} = [y_1, y_2, \dots, y_N]^T$ . The transfer function is given by:

$$H(z) = \frac{Y(z)}{X(z)} = \frac{b_0 + b_1 z^{-1} + \dots + b_{M-1} z^{-(M-1)}}{1 + a_1 z^{-1} + \dots + a_{N-1} z^{-(N-1)}} \quad (2)$$

where  $b_k$  and  $a_k$  are the coefficients of the numerator and denominator polynomials, respectively, and  $M$  and  $N$  are the orders of the numerator and denominator polynomials.

The input signal  $x[n]$  is assumed to be a white noise process with zero mean and unit variance. The output signal  $y[n]$  is then given by:

$$y[n] = \sum_{k=0}^{M-1} b_k x[n-k] + \sum_{k=0}^{N-1} a_k y[n-k] \quad (3)$$

Equation (3) can be rearranged to give the difference equation for the system:

$$y[n] - \sum_{k=0}^{N-1} a_k y[n-k] = \sum_{k=0}^{M-1} b_k x[n-k] \quad (4)$$

where  $a_k$  and  $b_k$  are the coefficients of the denominator and numerator polynomials, respectively. The system is assumed to be causal and stable, which implies that  $|a_k| < 1$  and  $|b_k| < 1$  for all  $k$ .

On the

It has been shown that the output signal  $y[n]$  is a stationary process with a power spectrum given by:

$$S_y(\omega) = |H(e^{j\omega})|^2 S_x(\omega) \quad (5)$$

where  $S_x(\omega)$  is the power spectrum of the input signal  $x[n]$ , which is assumed to be white noise with a constant power spectrum  $S_x(\omega) = 1$ . The power spectrum of the output signal  $y[n]$  is then given by:

$$S_y(\omega) = |H(e^{j\omega})|^2 \quad (6)$$

where  $H(e^{j\omega})$  is the frequency response of the system, given by:

$$H(e^{j\omega}) = \frac{b_0 + b_1 e^{-j\omega} + \dots + b_{M-1} e^{-j\omega(M-1)}}{1 + a_1 e^{-j\omega} + \dots + a_{N-1} e^{-j\omega(N-1)}} \quad (7)$$

The output signal  $y[n]$  is then assumed to be a white noise process with a constant power spectrum  $S_y(\omega) = 1$ . The power spectrum of the input signal  $x[n]$  is then given by:

$$S_x(\omega) = \frac{1}{|H(e^{j\omega})|^2} \quad (8)$$

ing. In the case of the first two, the same re-

ferences

1. Applied in the case of the High
2. In the case of the survey (HRES) done by Search for Battle
3. In the case of the High in the case of the mapping at
4. In the case of the High in the case of the mapping at
5. In the case of the High in the case of the mapping at
6. In the case of the High in the case of the mapping at
7. In the case of the High in the case of the mapping at
8. In the case of the High in the case of the mapping at
9. In the case of the High in the case of the mapping at
10. In the case of the High in the case of the mapping at

High

1. In the case of the High in the case of the mapping at
2. In the case of the High in the case of the mapping at
3. In the case of the High in the case of the mapping at
4. In the case of the High in the case of the mapping at
5. In the case of the High in the case of the mapping at
6. In the case of the High in the case of the mapping at
7. In the case of the High in the case of the mapping at
8. In the case of the High in the case of the mapping at
9. In the case of the High in the case of the mapping at
10. In the case of the High in the case of the mapping at

In the case of the High in the case of the mapping at